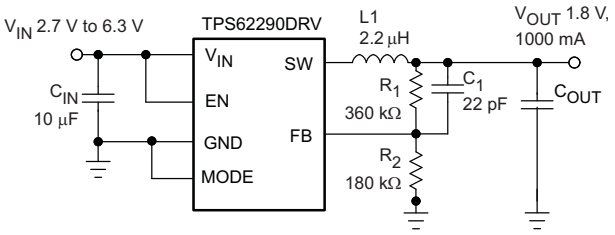
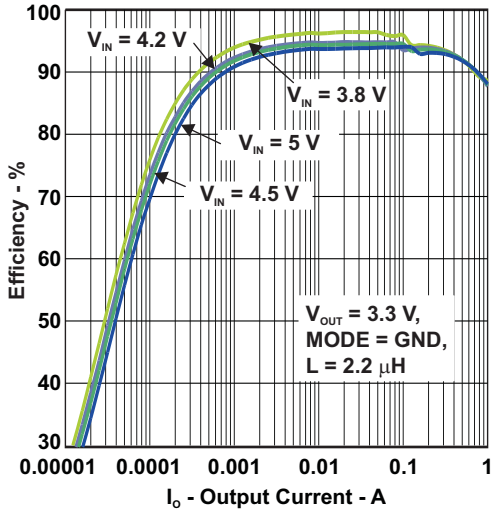
1-A Step Down Converter in 2 x 2 SON Package

Check for Samples: TPS62290-Q1, TPS62291-Q1, TPS62293-Q1

FEATURES

- **Qualified for Automotive Applications**
- **High Efficiency Step Down Converter**
- **Output Current up to 1000 mA**
- **V_{IN} Range From 2.3 V to 6 V**
- **2.25 MHz Fixed Frequency Operation**
- **Power Save Mode at Light Load Currents**
- **Output Voltage Accuracy in PWM mode ±1.5%**
- **Fixed Output Voltage Options**
- **Typ. 15-µA Quiescent Current**
- **100% Duty Cycle for Lowest Dropout**
- **Voltage Positioning at Light Loads**
- **Available in a 2 × 2 × 0,8 mm SON Package**





DESCRIPTION

The TPS6229x-Q1 is a highly efficient synchronous step down dc-dc converters optimized for battery-powered portable applications. TPS6229x-Q1 provides up to 1000-mA output current from a single Li-Ion cell.

With an input voltage range of 2.3 V to 6 V, the device supports batteries with extended voltage range and are ideal to power portable applications like mobile phones and other portable equipment.

The TPS6229x-Q1 operates at 2.25-MHz fixed switching frequency and enters Power Save Mode operation at light load currents to maintain high efficiency over the entire load current range.

The Power Save Mode is optimized for low output voltage ripple. For low noise applications, the device can be forced into fixed frequency PWM mode by pulling the MODE pin high. In the shutdown mode, the current consumption is reduced to less than 1 µA. The TPS6229x-Q1 allows the use of small inductors and capacitors to achieve a small solution size.

The TPS6229x-Q1 is available in a 2-mm × 2-mm 6-pin SON package.

ABSOLUTE MAXIMUM RATINGS

over operating free-air temperature range (unless otherwise noted)(1)

		VALUE	UNIT
V_I	Input voltage range(2)	–0.3 to 7	V
	Voltage range at EN, MODE	–0.3 to V_{IN} +0.3, ≤ 7	
	Voltage on SW	–0.3 to 7	
	Peak output current	Internally limited	A
T_J	Maximum operating junction temperature	–40 to 125	°C
T_{stg}	Storage temperature range	–65 to 150	

(1) Stresses beyond those listed under *absolute maximum ratings* may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other conditions beyond those indicated under *recommended operating conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
(2) All voltage values are with respect to network ground terminal.

DISSIPATION RATINGS

PACKAGE	$R_{\theta JA}$	POWER RATING FOR $T_A \le 25°C$	DERATING FACTOR ABOVE $T_A = 25°C$
DRV	76°C/W	1300 mW	13 mW/°C

RECOMMENDED OPERATING CONDITIONS

			MIN	NOM	MAX	UNIT
V_{IN}	Supply voltage		2.3		6	V
	Output voltage range for adjustable voltage		0.6		VIN	V
T_A	Operating ambient temperature	TPS62290IDRVRQ1	–40		85	°C
		TPS6229XTDRVRQ1	–40		105	
T_J	Operating junction temperature		–40		125	°C

ELECTRICAL CHARACTERISTICS

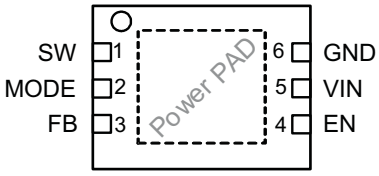
Over full operating ambient temperature range, typical values are at T_A = 25°C. Unless otherwise noted, specifications apply for condition V_{IN} = EN = 3.6V. External components C_{IN} = 4.7µF 0603, C_{OUT} = 10µF 0603, L = 2.2µH, refer to parameter measurement information.

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
SUPPLY							
V_I	Input voltage range			2.3		6	V
I_O	Output current(1)	V_{IN} 2.7 V to 6 V				1000	mA
		V_{IN} 2.5 V to 2.7 V				600	
		V_{IN} 2.3 V to 2.5 V				300	
I_Q	Operating quiescent current	I_O = 0 mA, PFM mode enabled (MODE = GND) device not switching, See (2)			15		µA
		I_O = 0 mA, switching with no load, (MODE = V_{IN}) PWM operation, V_O = 1.8 V, V_{IN} = 3V			3.8		mA
I_{SD}	Shutdown current	EN = GND	T_A = 25°C		0.1	1	µA
			T_A = 105°C			2.5	
UVLO	Undervoltage lockout threshold	Falling			1.85		V
		Rising			1.95		
ENABLE, MODE							
V_{IH}	High level input voltage, EN, MODE	2.3 V ≤ V_{IN} ≤ 6 V		1		V_{IN}	V
V_{IL}	Low level input voltage, EN, MODE	2.3 V ≤ V_{IN} ≤ 6 V		0		0.4	V
I_I	Input bias current, EN, MODE	EN, MODE = GND or V_{IN}			0.01	1	µA
POWER SWITCH							
$R_{DS(on)}$	High side MOSFET on-resistance	V_{IN} = V_{GS} = 3.6 V, T_A = 25°C			240	480	mΩ
	Low side MOSFET on-resistance				185	380	
I_{LIMF}	Forward current limit MOSFET high-side and low side	V_{IN} = V_{GS} = 3.6 V, T_A = 25°C		1.19	1.4	1.78	A
T_{SD}	Thermal shutdown	Increasing junction temperature			140		°C
	Thermal shutdown hysteresis	Decreasing junction temperature			20		
OSCILLATOR							
f_{SW}	Oscillator frequency	2.3 V ≤ V_{IN} ≤ 6 V		2.0	2.25	2.5	MHz
OUTPUT							
V_O	Adjustable output voltage range			0.6		V_I	V
V_{ref}	Reference voltage				600		mV
$V_{FB(PWM)}$	Feedback voltage	MODE = V_{IN}, PWM operation, 2.3 V ≤ V_{IN} ≤ 6 V, See (3)		–1.5	0	1.5	%
$V_{FB(PFM)}$	Feedback voltage PFM mode	MODE = GND, device in PFM mode, +1% voltage positioning active, See (2)			1		
	Load regulation				- 0.5		%/A
$t_{Start\ Up}$	Start-up time	Time from active EN to reach 95% of V_O			500		µs
t_{Ramp}	V_O ramp-up time	Time to ramp from 5% to 95% of V_O			250		µs
I_{lkg}	Leakage current into SW pin	V_I = 3.6 V, V_I = V_O = V_{SW}, EN = GND, See (4)			0.1	1	µA

(1) Not Production Tested.
(2) In PFM mode, the internal reference voltage is set to typ. 1.01 × V_{ref} . See the parameter measurement information.
(3) For V_{IN} = V_O + 1.0 V
(4) In fixed output voltage versions, the internal resistor divider network is disconnected from FB pin.

PIN ASSIGNMENTS

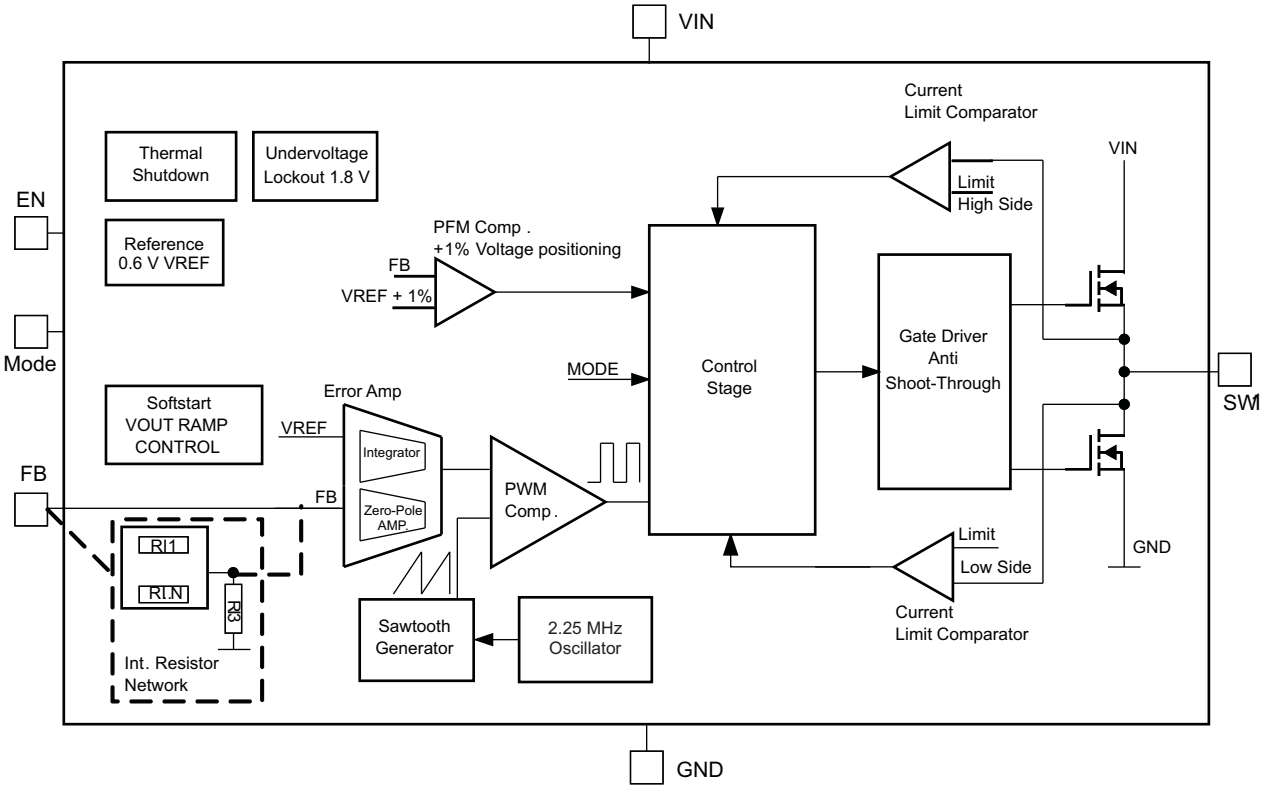
DRV PACKAGE
(TOP VIEW)



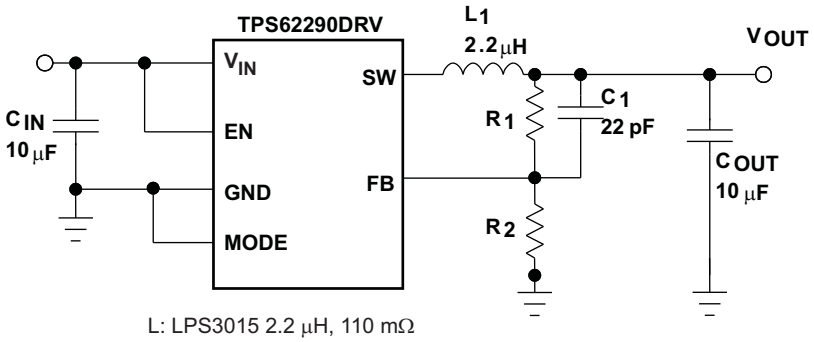
TERMINAL FUNCTIONS

TERMINAL		I/O	DESCRIPTION
NAME	NO.		
V_{IN}	5	PWR	VIN power supply pin.
GND	6	PWR	GND supply pin
EN	4	I	This is the enable pin of the device. Pulling this pin to low forces the device into shutdown mode. Pulling this pin to high enables the device. This pin must be terminated.
SW	1	OUT	This is the switch pin and is connected to the internal MOSFET switches. Connect the external inductor between this terminal and the output capacitor.
FB	3	I	Feedback Pin for the internal regulation loop. Connect the external resistor divider to this pin. In case of fixed output voltage option, connect this pin directly to the output capacitor
MODE	2	I	MODE pin = high forces the device to operate in fixed-frequency PWM mode. Mode pin = low enables the Power Save Mode with automatic transition from PFM mode to fixed-frequency PWM mode.

FUNCTIONAL BLOCK DIAGRAM



PARAMETER MEASUREMENT INFORMATION



L: LPS3015 2.2 µH, 110 mΩ
C_{IN}: GRM188R60J106M 10 µF Murata 0603 size
C_{OUT}: GRM188R60J106M 10 µF Murata 0603 size

TYPICAL CHARACTERISTICS

Table 1. Table Of Graphs

		FIGURE
Efficiency	vs V_O 1.8 V Power Save Mode	Figure 1
Efficiency	vs V_O 1.8 V Forced Save Mode	Figure 2
Efficiency	vs V_O 3.3 V Power Save Mode	Figure 3
Efficiency	vs V_O 3.3 V Forced Save Mode	Figure 4
V_O ACCURACY		Figure 5
V_O ACCURACY		Figure 8
V_O ACCURACY		Figure 7
V_O ACCURACY		Figure 6
PFM LOAD TRANSIENT		Figure 9
PFM LINE TRANSIENT		Figure 10
PWM LOAD TRANSIENT		Figure 11
PWM LINE TRANSIENT		Figure 12
TYPICAL OPERATION PFM MODE		Figure 13
TYPICAL OPERATION PWM MODE		Figure 14
Shutdown Current Into VIN	vs Input Voltage, (T_A = 85°C, T_A = 25°C, T_A = -40°C)	Figure 15
Quiescent Current	vs Input Voltage, (T_A = 85°C, T_A = 25°C, T_A = -40°C)	Figure 16
Static Drain-Source On-State Resistance	vs Input Voltage, (T_A = 85°C, T_A = 25°C, T_A = -40°C)	Figure 17 Figure 18

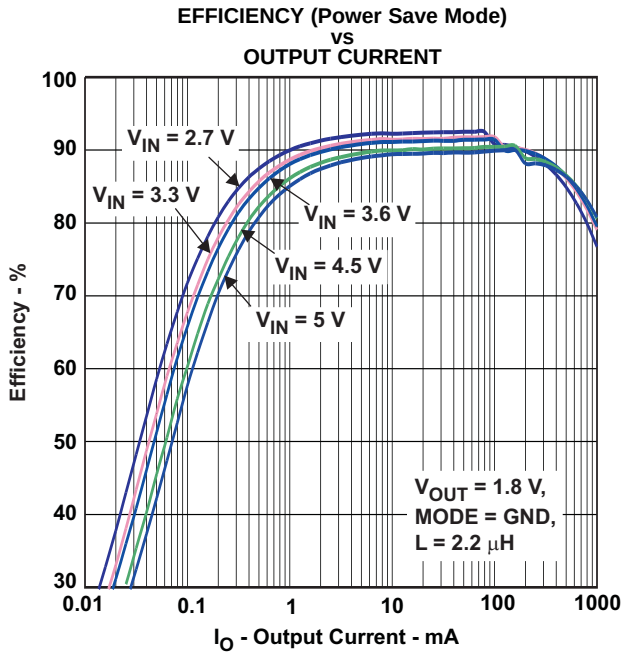


Figure 1.

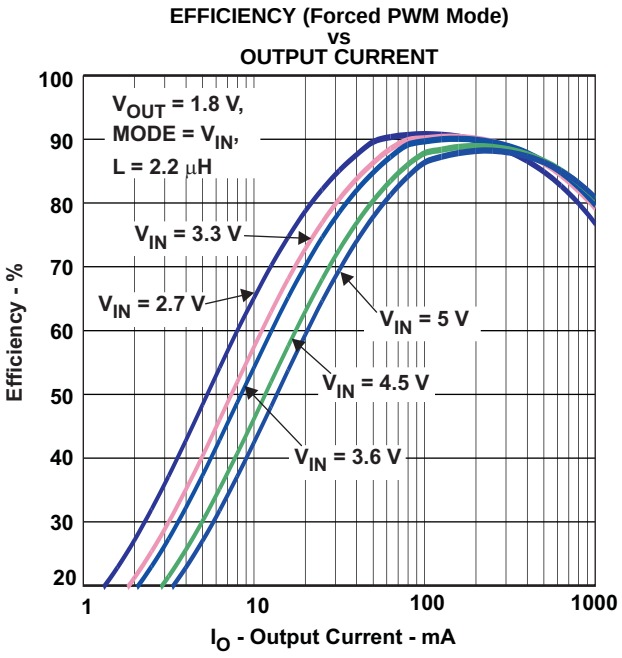


Figure 2.

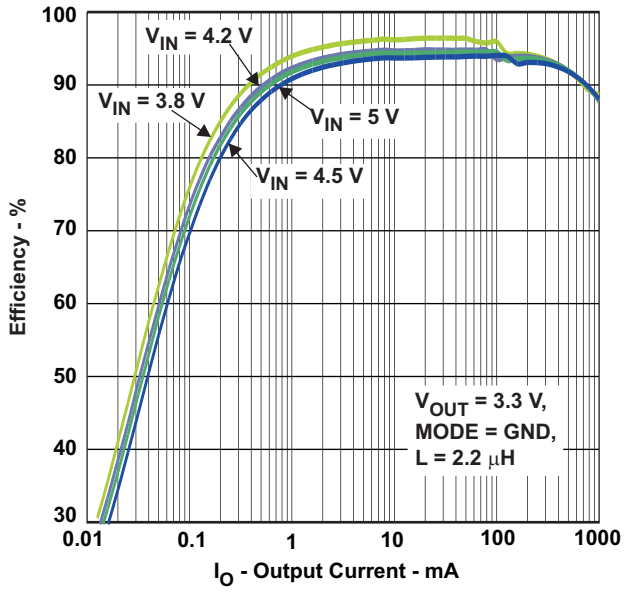


Figure 3.

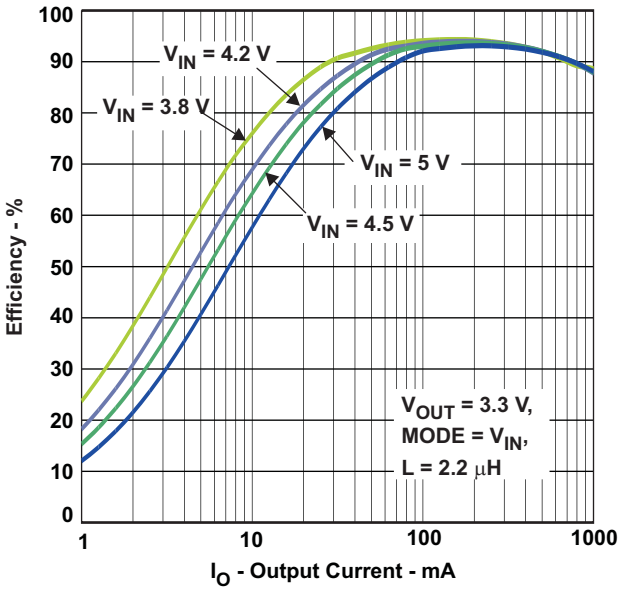


Figure 4.

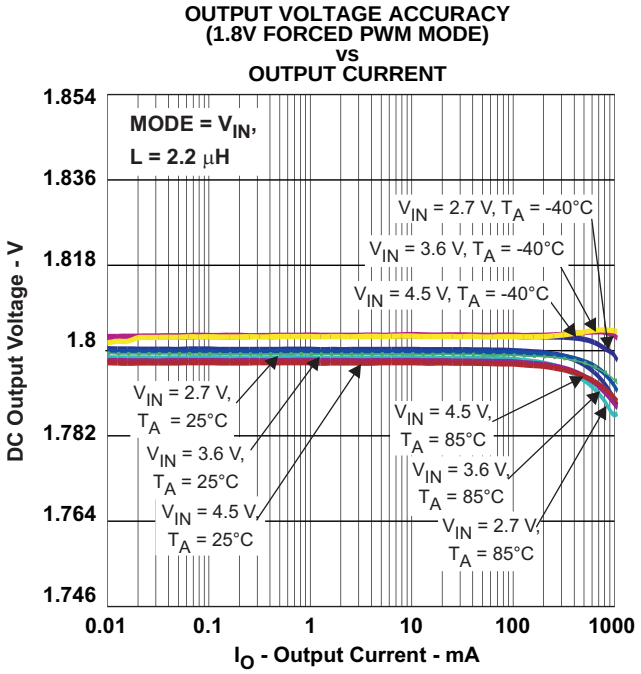


Figure 5.

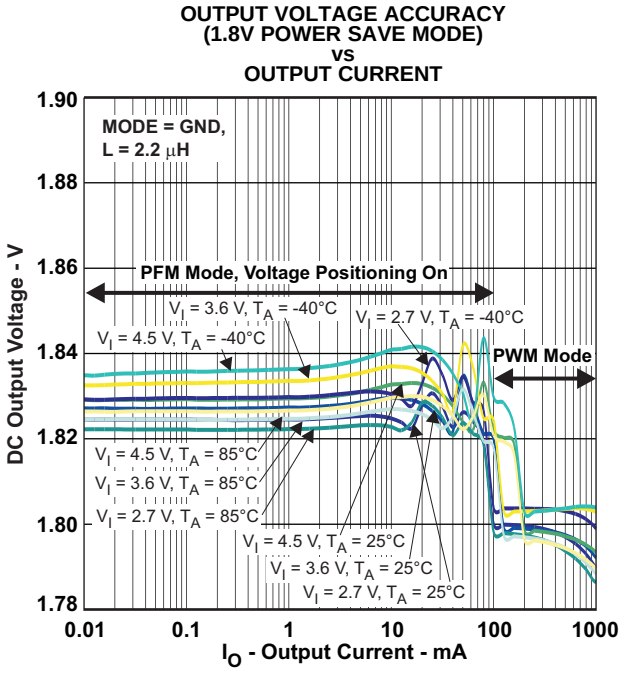


Figure 6.

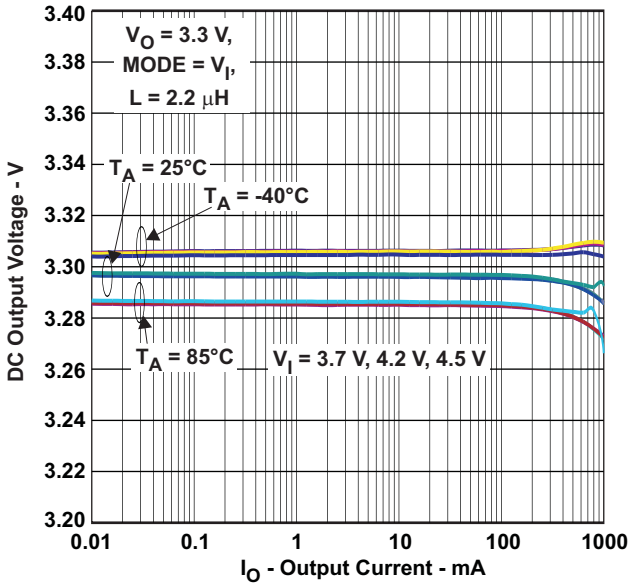


Figure 7.

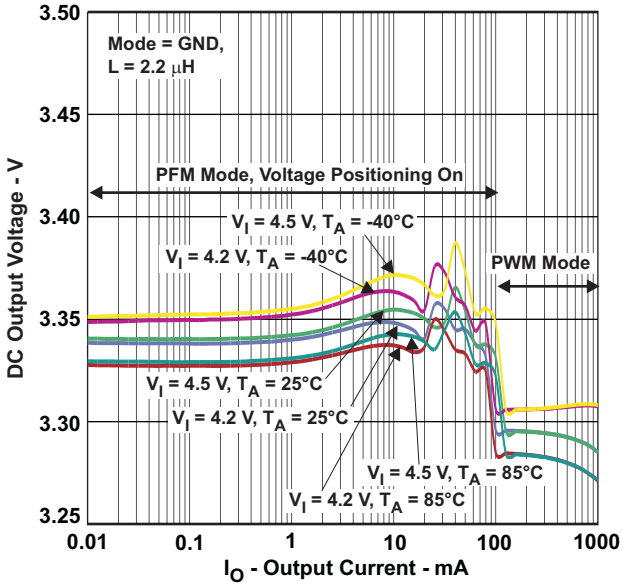
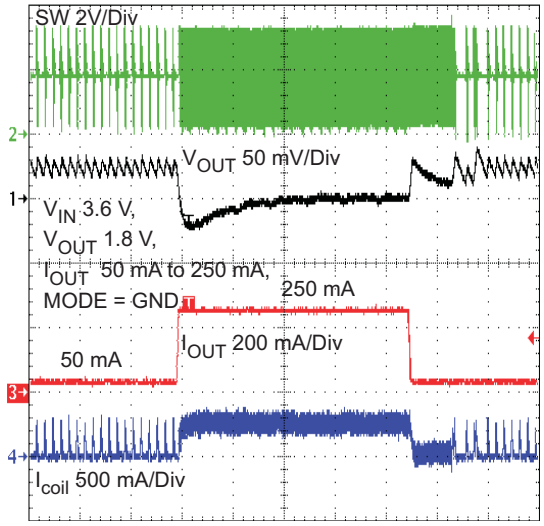


Figure 8.

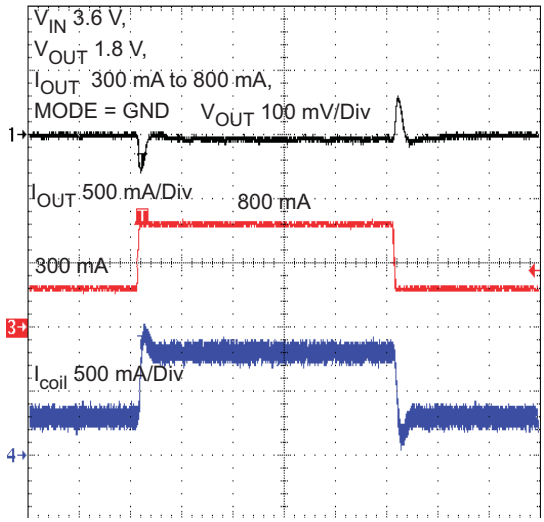
PFM LOAD TRANSIENT



Time Base - 20 µs/Div

Figure 9.

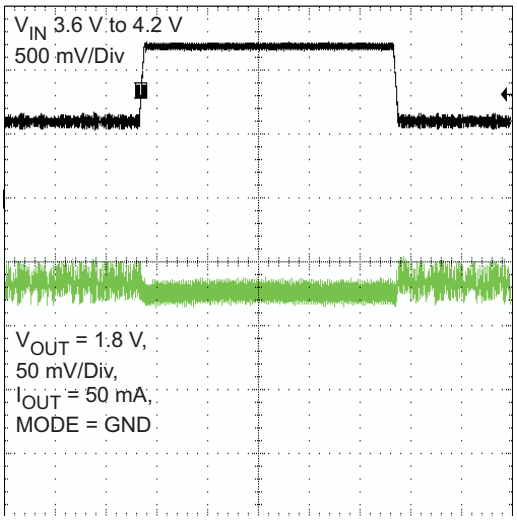
PFM LINE TRANSIENT



Time Base - 20 µs/Div

Figure 10.

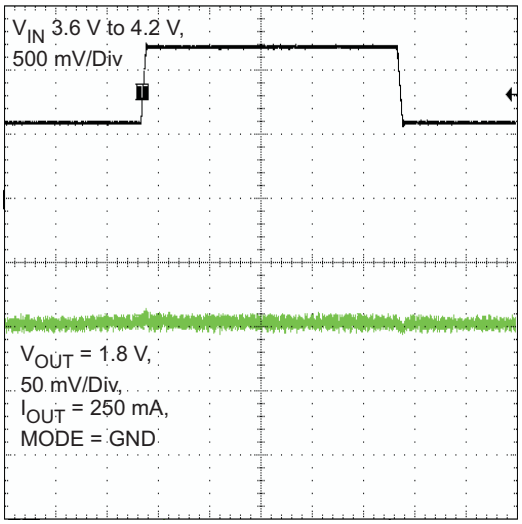
PWM LOAD TRANSIENT



Time Base - 100 µs/Div

Figure 11.

PWM LINE TRANSIENT



Time Base - 100 µs/Div

Figure 12.

TYPICAL OPERATION VS PFM MODE

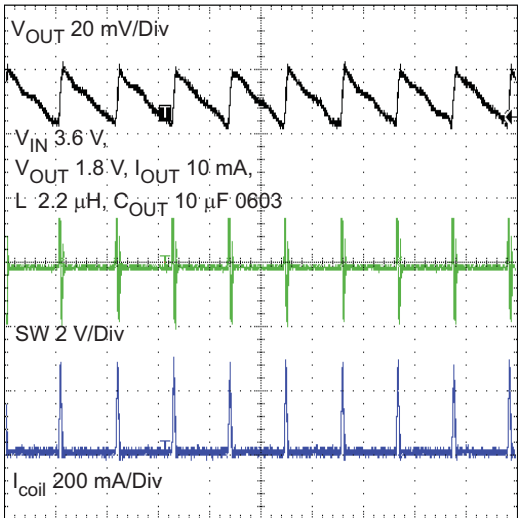


Figure 13.

TYPICAL OPERATION VS PWM MODE

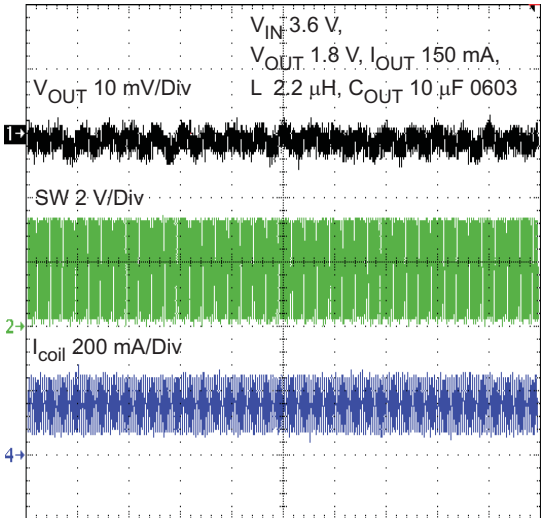


Figure 14.

SHUTDOWN CURRENT INTO VIN VS INPUT VOLTAGE

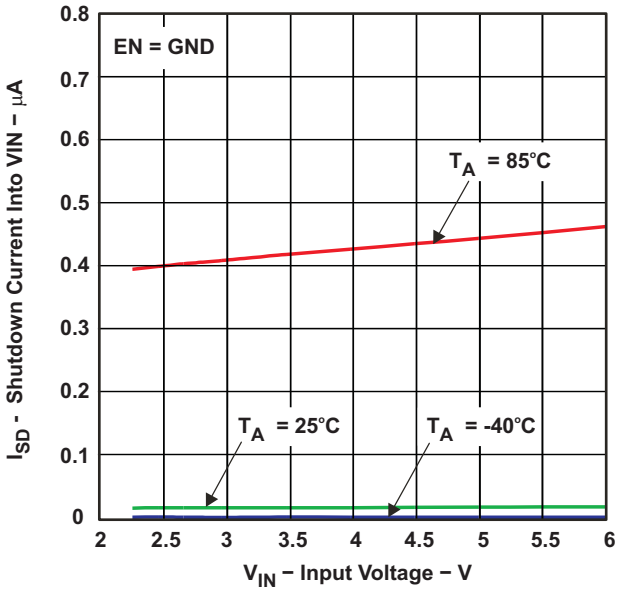


Figure 15.

QUIESCENT CURRENT VS INPUT VOLTAGE

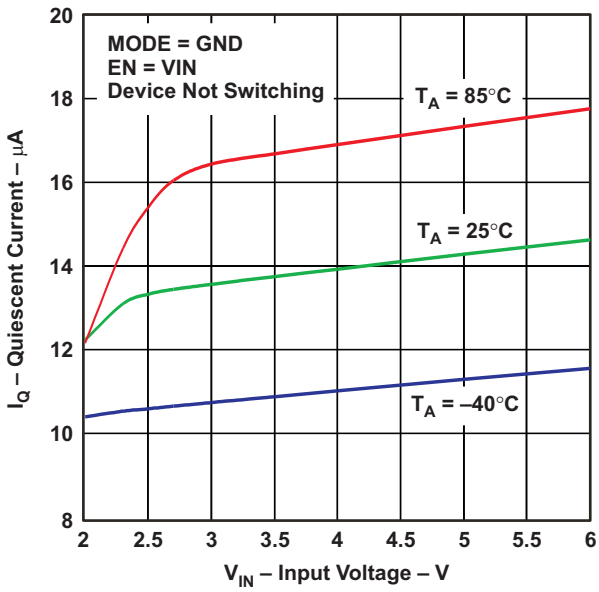


Figure 16.

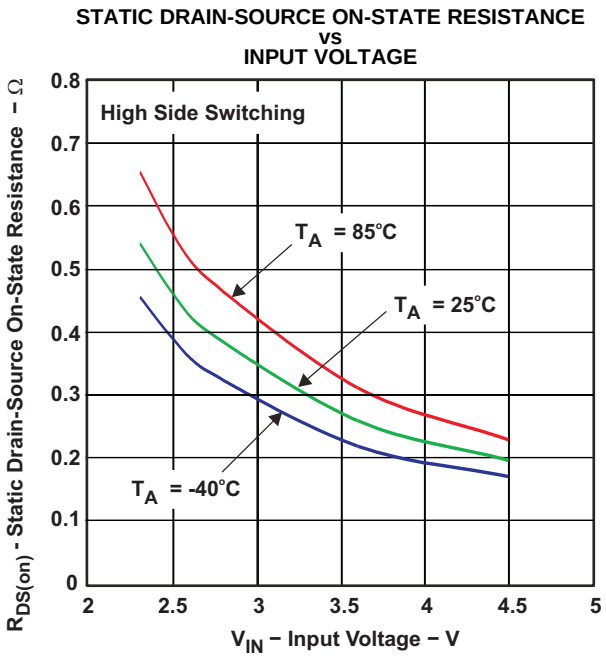


Figure 17.

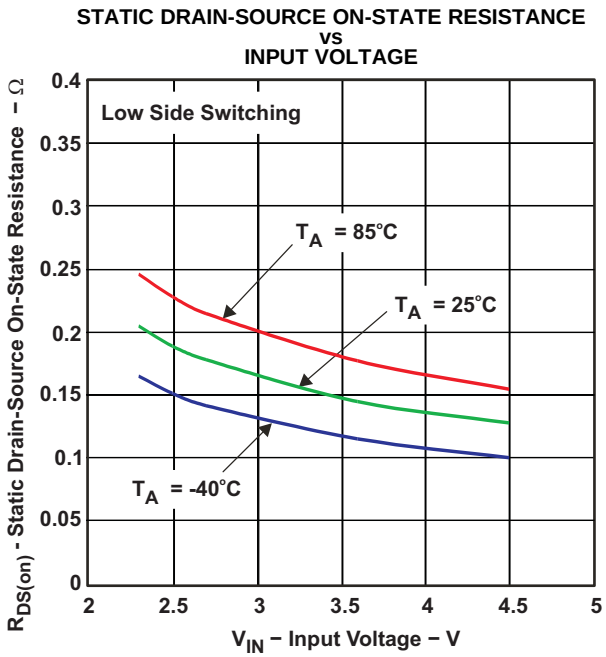


Figure 18.

DETAILED DESCRIPTION

OPERATION

The TPS6229x-Q1 step down converter operates with typically 2.25-MHz fixed frequency pulse width modulation (PWM) at moderate to heavy load currents. At light load currents, the converter can automatically enter Power Save Mode and operates then in PFM mode.

During PWM operation, the converter use a unique fast response voltage mode controller scheme with input voltage feed-forward to achieve good line and load regulation allowing the use of small ceramic input and output capacitors. At the beginning of each clock cycle initiated by the clock signal, the High Side MOSFET switch is turned on. The current flows now from the input capacitor via the High Side MOSFET switch through the inductor to the output capacitor and load. During this phase, the current ramps up until the PWM comparator trips and the control logic turns off the switch. The current limit comparator also turns off the switch if the current limit of the High Side MOSFET switch is exceeded. After a dead time preventing shoot through current, the Low Side MOSFET rectifier is turned on and the inductor current ramps down. The current flows now from the inductor to the output capacitor and to the load. It returns to the inductor through the Low Side MOSFET rectifier.

The next cycle is initiated by the clock signal again turning off the Low Side MOSFET rectifier and turning on the on the High Side MOSFET switch.

POWER SAVE MODE

The Power Save Mode is enabled with MODE Pin set to low level. If the load current decreases, the converter will enter Power Save Mode operation automatically. During Power Save Mode the converter skips switching and operates with reduced frequency in PFM mode with a minimum quiescent current to maintain high efficiency. The converter will position the output voltage typically +1% above the nominal output voltage. This voltage positioning feature minimizes voltage drops caused by a sudden load step.

The transition from PWM mode to PFM mode occurs once the inductor current in the Low Side MOSFET switch becomes zero, which indicates discontinuous conduction mode.

During the Power Save Mode the output voltage is monitored with a PFM comparator. As the output voltage falls below the PFM comparator threshold of VOUT nominal +1%, the device starts a PFM current pulse. For this the High Side MOSFET switch will turn on and the inductor current ramps up. After the On-time expires, the switch is turned off and the Low Side MOSFET switch is turned on until the inductor current becomes zero.

The converter effectively delivers a current to the output capacitor and the load. If the load is below the delivered current, the output voltage will rise. If the output voltage is equal or higher than the PFM comparator threshold, the device stops switching and enters a sleep mode with typical 15µA current consumption.

If the output voltage is still below the PFM comparator threshold, a sequence of further PFM current pulses are generated until the PFM comparator threshold is reached. The converter starts switching again once the output voltage drops below the PFM comparator threshold.

With a fast single threshold comparator, the output voltage ripple during PFM mode operation can be kept small. The PFM Pulse is time controlled, which allows to modify the charge transferred to the output capacitor by the value of the inductor. The resulting PFM output voltage ripple and PFM frequency depend in first order on the size of the output capacitor and the inductor value. Increasing output capacitor values and inductor values will minimize the output ripple. The PFM frequency decreases with smaller inductor values and increases with larger values.

The PFM mode is left and PWM mode entered in case the output current can not longer be supported in PFM mode. The Power Save Mode can be disabled through the MODE pin set to high. The converter will then operate in fixed frequency PWM mode.

Dynamic Voltage Positioning

This feature reduces the voltage under/overshoots at load steps from light to heavy load and vice versa. It is active in Power Save Mode and regulates the output voltage 1% higher than the nominal value. This provides more headroom for both the voltage drop at a load step, and the voltage increase at a load throw-off.

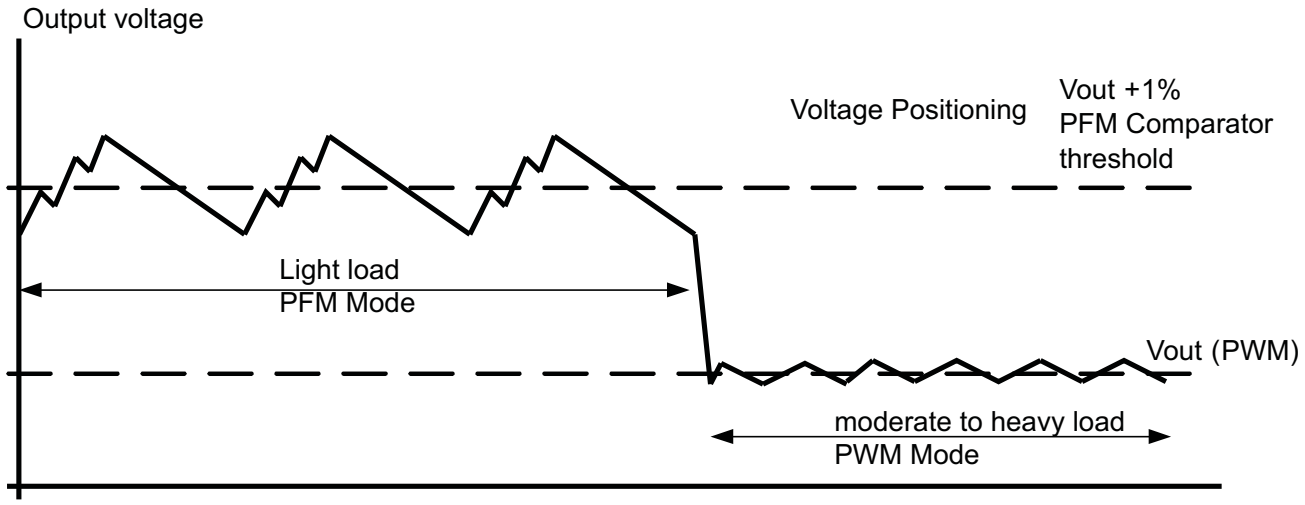


Figure 19. Power Save Mode Operation

100% Duty Cycle Low Dropout Operation

The device starts to enter 100% duty cycle Mode once the input voltage comes close the nominal output voltage. To maintain the output voltage, the High Side MOSFET switch is turned on 100% for one or more cycles.

With further decreasing VIN the High Side MOSFET switch is turned on completely. In this case, the converter offers a low input-to-output voltage difference. This is particularly useful in battery-powered applications to achieve longest operation time by taking full advantage of the whole battery voltage range.

The minimum input voltage to maintain regulation depends on the load current and output voltage, and can be calculated as:

$V_{IN}min = V_O max + I_O max \times R_{DS(on)} max + R_L)$

With:

$I_O max$ = maximum output current plus inductor ripple current

$R_{DS(on)} max$ = maximum P-channel switch $R_{DS(on)}$.

R_L = DC resistance of the inductor

$V_O max$ = nominal output voltage plus maximum output voltage tolerance

Undervoltage Lockout

The undervoltage lockout circuit prevents the device from malfunctioning at low input voltages and from excessive discharge of the battery and disables the output stage of the converter. The undervoltage lockout threshold is typically 1.85V with falling V_{IN}.

MODE SELECTION

The MODE pin allows mode selection between forced PWM mode and Power Save Mode.

Connecting this pin to GND enables the Power Save Mode with automatic transition between PWM and PFM mode. Pulling the MODE pin high forces the converter to operate in fixed frequency PWM mode even at light load currents. This allows simple filtering of the switching frequency for noise sensitive applications. In this mode, the efficiency is lower compared to the power save mode during light loads.

The condition of the MODE pin can be changed during operation and allows efficient power management by adjusting the operation mode of the converter to the specific system requirements.

ENABLE

The device is enabled setting EN pin to high. During the start up time $t_{Start\ Up}$ the internal circuits are settled. Afterwards, the device activates the soft start circuit. The EN input can be used to control power sequencing in a system with various dc/dc converters. The EN pin can be connected to the output of another converter, to drive the EN pin high and getting a sequencing of supply rails. With EN = GND, the device enters shutdown mode. In this mode, all circuits are disabled. In fixed output voltage versions, the internal resistor divider network is disconnected from FB pin.

SOFT START

The TPS6229x-Q1 has an internal soft start circuit that controls the ramp up of the output voltage. The output voltage ramps up from 5% to 95% of its nominal value within typical 250µs. This limits the inrush current in the converter during ramp up and prevents possible input voltage drops when a battery or high impedance power source is used. The soft start circuit is enabled within the start up time $t_{Start\ Up}$.

SHORT-CIRCUIT PROTECTION

The High Side and Low Side MOSFET switches are short-circuit protected with maximum switch current = I_{LIMF}. The current in the switches is monitored by current limit comparators. Once the current in the High Side MOSFET switch exceeds the threshold of it's current limit comparator, it turns off and the Low Side MOSFET switch is activated to ramp down the current in the inductor and High Side MOSFET switch. The High Side MOSFET switch can only turn on again, once the current in the Low Side MOSFET switch has decreased below the threshold of its current limit comparator.

THERMAL SHUTDOWN

As soon as the junction temperature, T_J, exceeds 140°C (typical) the device goes into thermal shutdown. In this mode, the High Side and Low Side MOSFETs are turned-off. The device continues its operation when the junction temperature falls below the thermal shutdown hysteresis.

APPLICATION INFORMATION

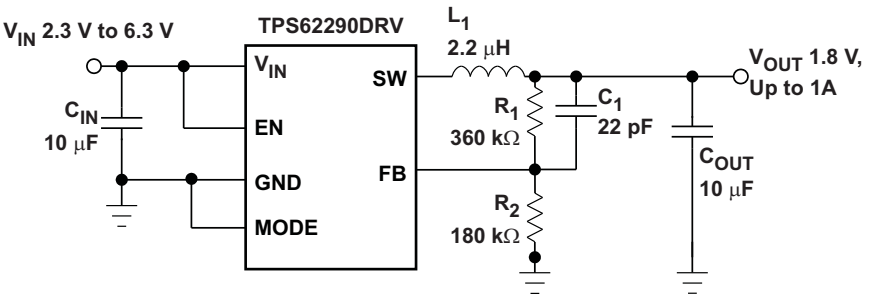


Figure 20. TPS62290DRV Adjustable 1.8 V

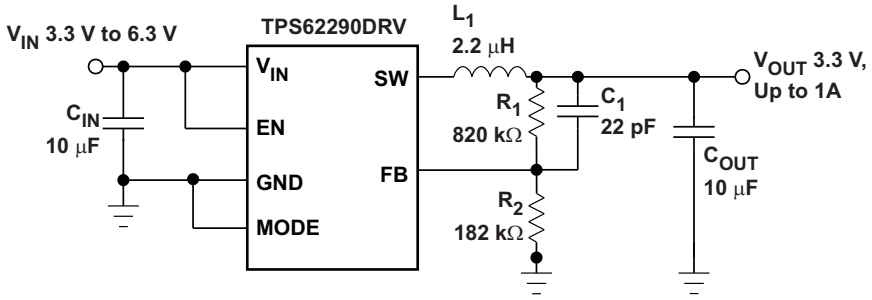


Figure 21. TPS62290DRV Adjustable 3.3 V

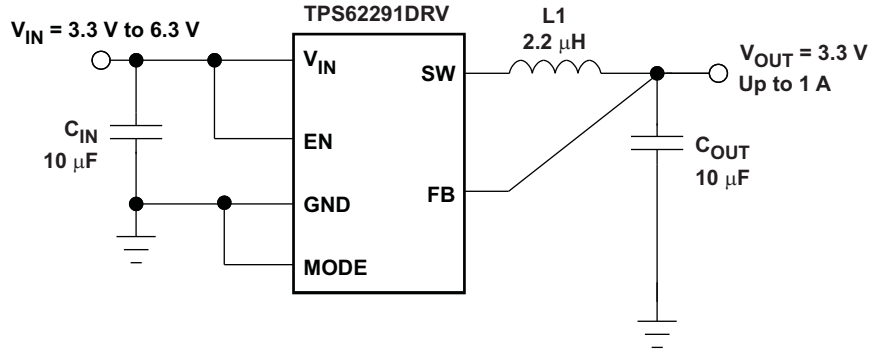


Figure 22.

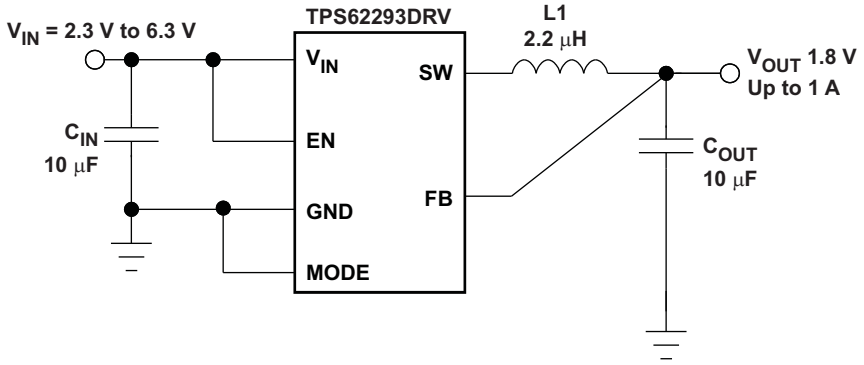


Figure 23.

OUTPUT VOLTAGE SETTING

The output voltage can be calculated to:

$$V_{OUT} = V_{REF} \times \left(1 + \frac{R_1}{R_2}\right)$$ with an internal reference voltage V_{REF} typical 0.6V.

To minimize the current through the feedback divider network, R_2 should be 180 kΩ or 360 kΩ. The sum of R_1 and R_2 should not exceed ~1MΩ, to keep the network robust against noise. An external feed forward capacitor C_1 is required for optimum load transient response. The value of C_1 should be in the range between 22pF and 33pF.

Route the FB line away from noise sources, such as the inductor or the SW line.

OUTPUT FILTER DESIGN (INDUCTOR AND OUTPUT CAPACITOR)

The TPS6229x-Q1 is designed to operate with inductors in the range of 1.5µH to 4.7µH and with output capacitors in the range of 4.7µF to 22µF. The part is optimized for operation with a 2.2µH inductor and 10µF output capacitor. Larger or smaller inductor values can be used to optimize the performance of the device for specific operation conditions. For stable operation, the L and C values of the output filter may not fall below 1µH effective inductance and 3.5µF effective capacitance.

Inductor Selection

The inductor value has a direct effect on the ripple current. The selected inductor has to be rated for its dc resistance and saturation current. The inductor ripple current (ΔI_L) decreases with higher inductance and increases with higher V_I or V_O.

The inductor selection has also impact on the output voltage ripple in PFM mode. Higher inductor values will lead to lower output voltage ripple and higher PFM frequency, lower inductor values will lead to a higher output voltage ripple but lower PFM frequency.

Equation 1 calculates the maximum inductor current under static load conditions. The saturation current of the inductor should be rated higher than the maximum inductor current as calculated with Equation 2. This is recommended because during heavy load transient the inductor current will rise above the calculated value.

$$\Delta I_L = V_{OUT} \times \frac{1 - \frac{V_{OUT}}{V_{IN}}}{L \times f} \quad (1)$$

$$I_L\,max = I_{out}\,max + \frac{\Delta I_L}{2} \quad (2)$$

With:

f = Switching Frequency (2.25MHz typical)

L = Inductor Value

ΔI_L = Peak to Peak inductor ripple current

I_{Lmax} = Maximum Inductor current

A more conservative approach is to select the inductor current rating just for the maximum switch current of the corresponding converter.

Accepting larger values of ripple current allows the use of low inductance values, but results in higher output voltage ripple, greater core losses, and lower output current capability.

The total losses of the coil have a strong impact on the efficiency of the dc/dc conversion and consist of both the losses in the dc resistance ($R_{(DC)}$) and the following frequency-dependent components:

- The losses in the core material (magnetic hysteresis loss, especially at high switching frequencies)
- Additional losses in the conductor from the skin effect (current displacement at high frequencies)
- Magnetic field losses of the neighboring windings (proximity effect)
- Radiation losses

Table 2. List of Inductors

DIMENSIONS [mm^3]	INDUCTOR TYPE	SUPPLIER
3 × 3 × 1.5	LPS3015	Coilcraft
3 x 3 x 1.5	LQH3NPN2R2NM0	MURATA
3.2 x 2.6 x 1.2	MIPSA3226D2R2	FDK

Output Capacitor Selection

The advanced fast-response voltage mode control scheme of the TPS6229x-Q1 allows the use of tiny ceramic capacitors. Ceramic capacitors with low ESR values have the lowest output voltage ripple and are recommended. The output capacitor requires either an X7R or X5R dielectric. Y5V and Z5U dielectric capacitors, aside from their wide variation in capacitance over temperature, become resistive at high frequencies.

At nominal load current, the device operates in PWM mode and the RMS ripple current is calculated as:

$$I_{RMSC_{OUT}} = V_{OUT} \times \frac{1 - \frac{V_{OUT}}{V_{IN}}}{L \times f} \times \frac{1}{2 \times \sqrt{3}} \quad (3)$$

At nominal load current, the device operates in PWM mode and the overall output voltage ripple is the sum of the voltage spike caused by the output capacitor ESR plus the voltage ripple caused by charging and discharging the output capacitor:

$$\Delta V_{OUT} = V_{OUT} \times \frac{1 - \frac{V_{OUT}}{V_{IN}}}{L \times f} \times \left(\frac{1}{8 \times Cout \times f} + ESR \right) \quad (4)$$

At light load currents the converter operates in Power Save Mode and the output voltage ripple is dependent on the output capacitor and inductor value. Larger output capacitor and inductor values minimize the voltage ripple in PFM mode and tighten dc output accuracy in PFM mode.

Input Capacitor Selection

The buck converter has a natural pulsating input current; therefore, a low ESR input capacitor is required for best input voltage filtering and minimizing the interference with other circuits caused by high input voltage spikes. For most applications, a 10-µF ceramic capacitor is recommended. The input capacitor can be increased without any limit for better input voltage filtering.

Take care when using only small ceramic input capacitors. When a ceramic capacitor is used at the input and the power is being supplied through long wires, such as from a wall adapter, a load step at the output or V_{IN} step on the input can induce ringing at the V_{IN} pin. The ringing can couple to the output and be mistaken as loop instability or could even damage the part by exceeding the maximum ratings.

Table 3. List of Capacitor

CAPACITANCE	TYPE	SIZE	SUPPLIER
10µF	GRM188R60J106M69D	0603 1.6x0.8x0.8mm3	Murata

LAYOUT CONSIDERATIONS

As for all switching power supplies, the layout is an important step in the design. Proper function of the device demands careful attention to PCB layout. Care must be taken in board layout to get the specified performance. If the layout is not carefully done, the regulator could show poor line and/or load regulation, stability issues as well as EMI problems. It is critical to provide a low inductance, impedance ground path. Therefore, use wide and short traces for the main current paths. The input capacitor should be placed as close as possible to the IC pins as well as the inductor and output capacitor.

Connect the GND Pin of the device to the Power Pad of the PCB and use this Pad as a star point. Use a common Power GND node and a different node for the Signal GND to minimize the effects of ground noise. Connect these ground nodes together to the Power Pad (star point) underneath the IC. Keep the common path to the GND PIN, which returns the small signal components and the high current of the output capacitors as short as possible to avoid ground noise. The FB line should be connected right to the output capacitor and routed away from noisy components and traces (e.g., SW line).

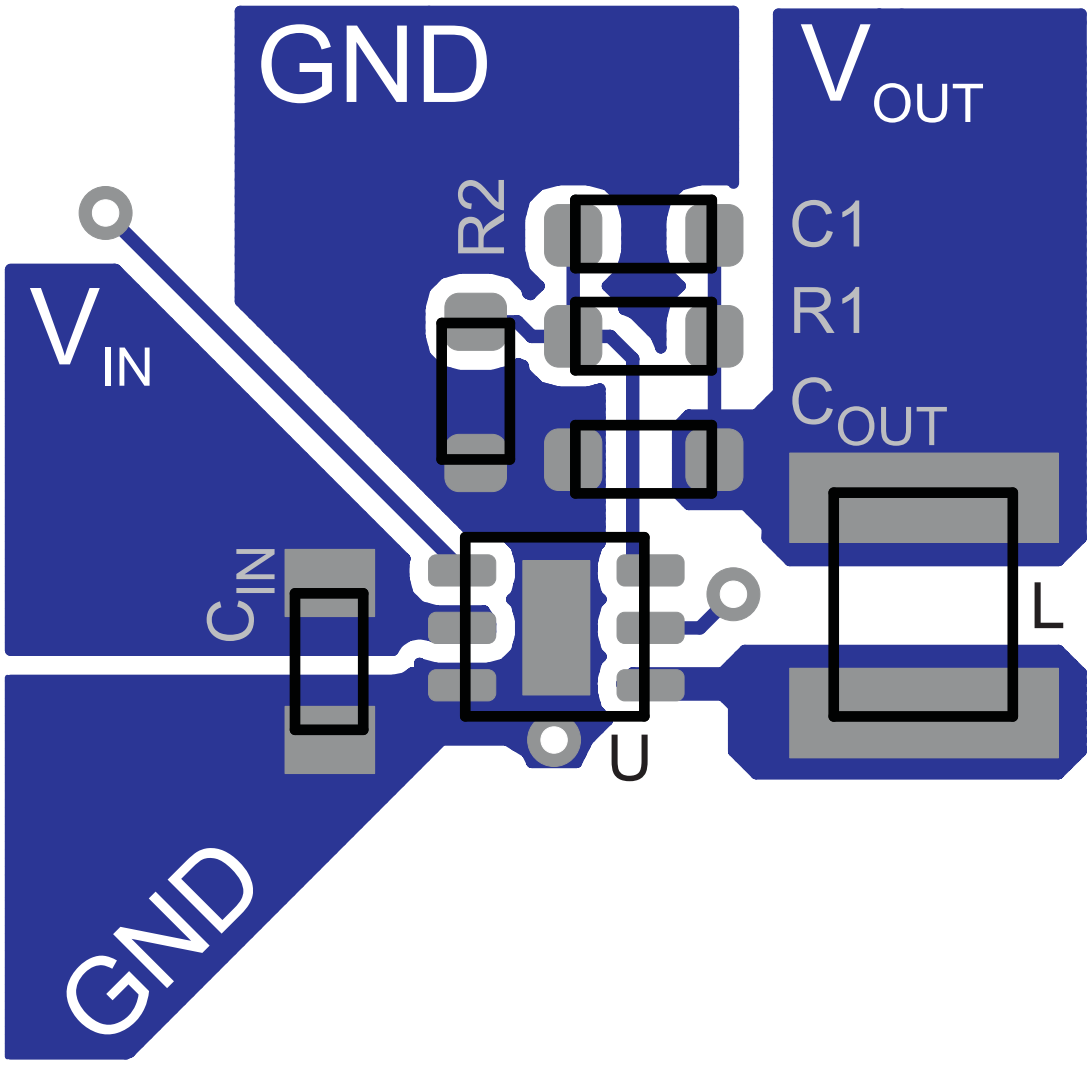


Figure 24. Layout

REVISION HISTORY

Changes from Original (April 2013) to Revision A	Page
• Deleted Ordering Information Table.	1

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish	MSL Peak Temp (3)	Op Temp (°C)	Top-Side Markings (4)	Samples
TPS62290IDRVRQ1	ACTIVE	SON	DRV	6	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	QVI	Samples
TPS62290TDRVRQ1	ACTIVE	SON	DRV	6	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	QVJ	Samples
TPS62293TDRVRQ1	ACTIVE	SON	DRV	6	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 105	QTO	Samples

(1) The marketing status values are defined as follows:
ACTIVE: Product device recommended for new designs.
LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.
NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.
PREVIEW: Device has been announced but is not in production. Samples may or may not be available.
OBSOLETE: TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check http://www.ti.com/productcontent for the latest availability information and additional product content details.
TBD: The Pb-Free/Green conversion plan has not been defined.
Pb-Free (RoHS): TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.
Pb-Free (RoHS Exempt): This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.
Green (RoHS & no Sb/Br): TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. -- The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) Multiple Top-Side Markings will be inside parentheses. Only one Top-Side Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Top-Side Marking for that device.

OTHER QUALIFIED VERSIONS OF TPS62290-Q1, TPS62293-Q1 :

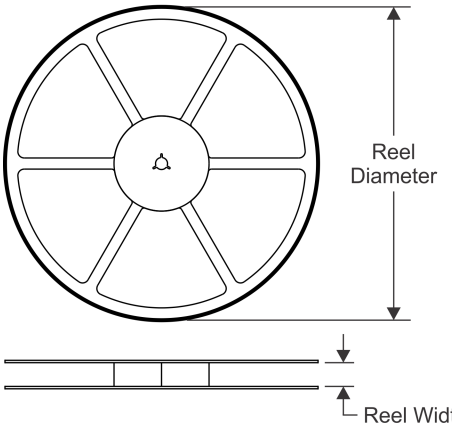
- Catalog: TPS62290, TPS62293

NOTE: Qualified Version Definitions:

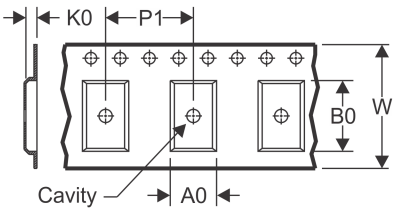
- Catalog - TI's standard catalog product

TAPE AND REEL INFORMATION

REEL DIMENSIONS

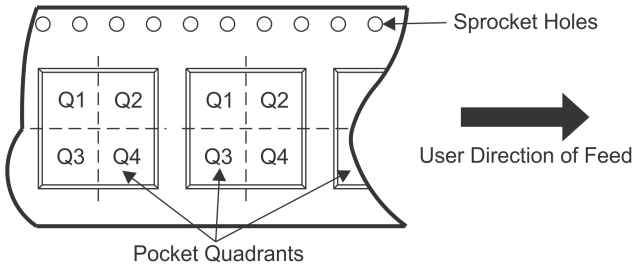


TAPE DIMENSIONS



A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

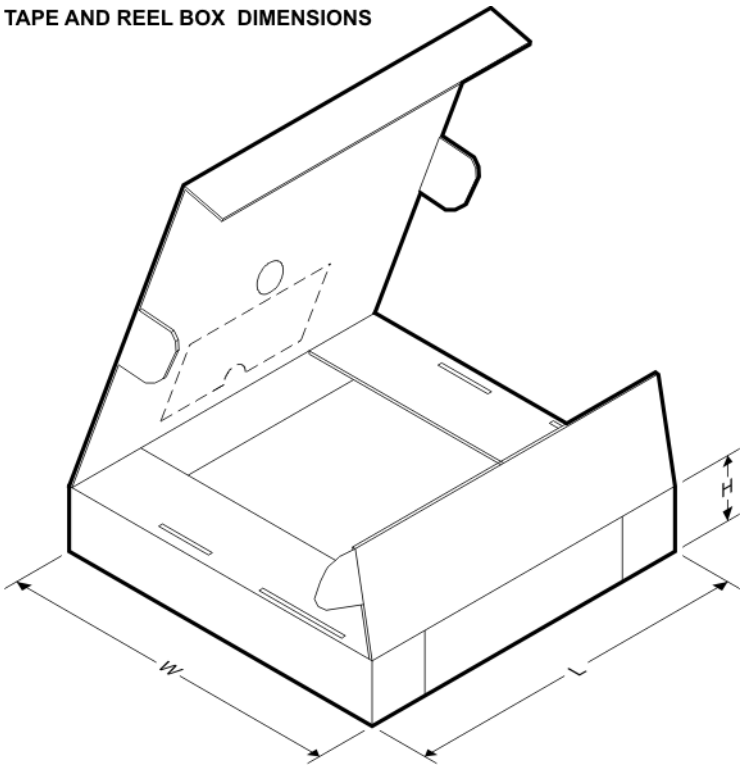
QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS62290IDRVRQ1	SON	DRV	6	3000	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2
TPS62290TDRVRQ1	SON	DRV	6	3000	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2
TPS62293TDRVRQ1	SON	DRV	6	3000	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2

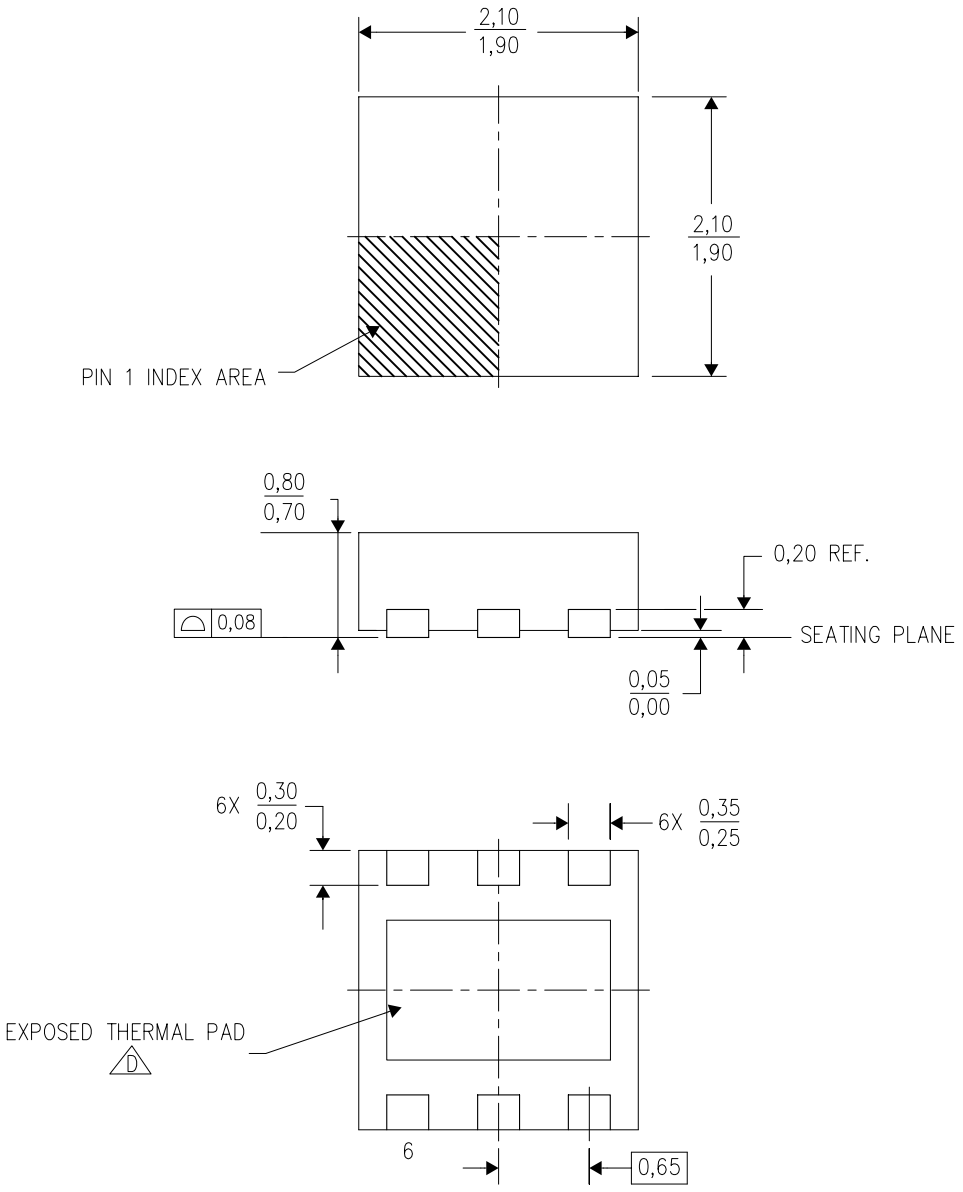
TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS62290IDRVRQ1	SON	DRV	6	3000	195.0	200.0	45.0
TPS62290TDRVRQ1	SON	DRV	6	3000	195.0	200.0	45.0
TPS62293TDRVRQ1	SON	DRV	6	3000	195.0	200.0	45.0

DRV (S–PWSON–N6) PLASTIC SMALL OUTLINE NO–LEAD



4206925/E 10/10

NOTES:
A. All linear dimensions are in millimeters. Dimensioning and tolerancing per ASME Y14.5M–1994.
B. This drawing is subject to change without notice.
C. Small Outline No–Lead (SON) package configuration.
D. The package thermal pad must be soldered to the board for thermal and mechanical performance. See the Product Data Sheet for details regarding the exposed thermal pad dimensions.

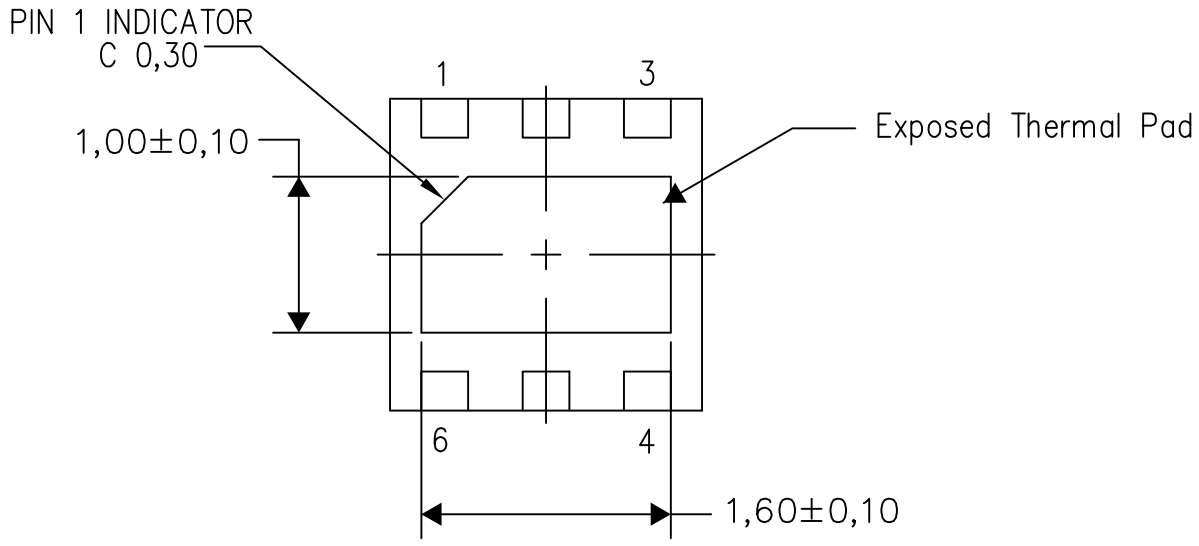
DRV (S–PWSON–N6) PLASTIC SMALL OUTLINE NO–LEAD

THERMAL INFORMATION

This package incorporates an exposed thermal pad that is designed to be attached directly to an external heatsink. The thermal pad must be soldered directly to the printed circuit board (PCB). After soldering, the PCB can be used as a heatsink. In addition, through the use of thermal vias, the thermal pad can be attached directly to the appropriate copper plane shown in the electrical schematic for the device, or alternatively, can be attached to a special heatsink structure designed into the PCB. This design optimizes the heat transfer from the integrated circuit (IC).

For information on the Quad Flatpack No–Lead (QFN) package and its advantages, refer to Application Report, QFN/SON PCB Attachment, Texas Instruments Literature No. SLUA271. This document is available at www.ti.com.

The exposed thermal pad dimensions for this package are shown in the following illustration.



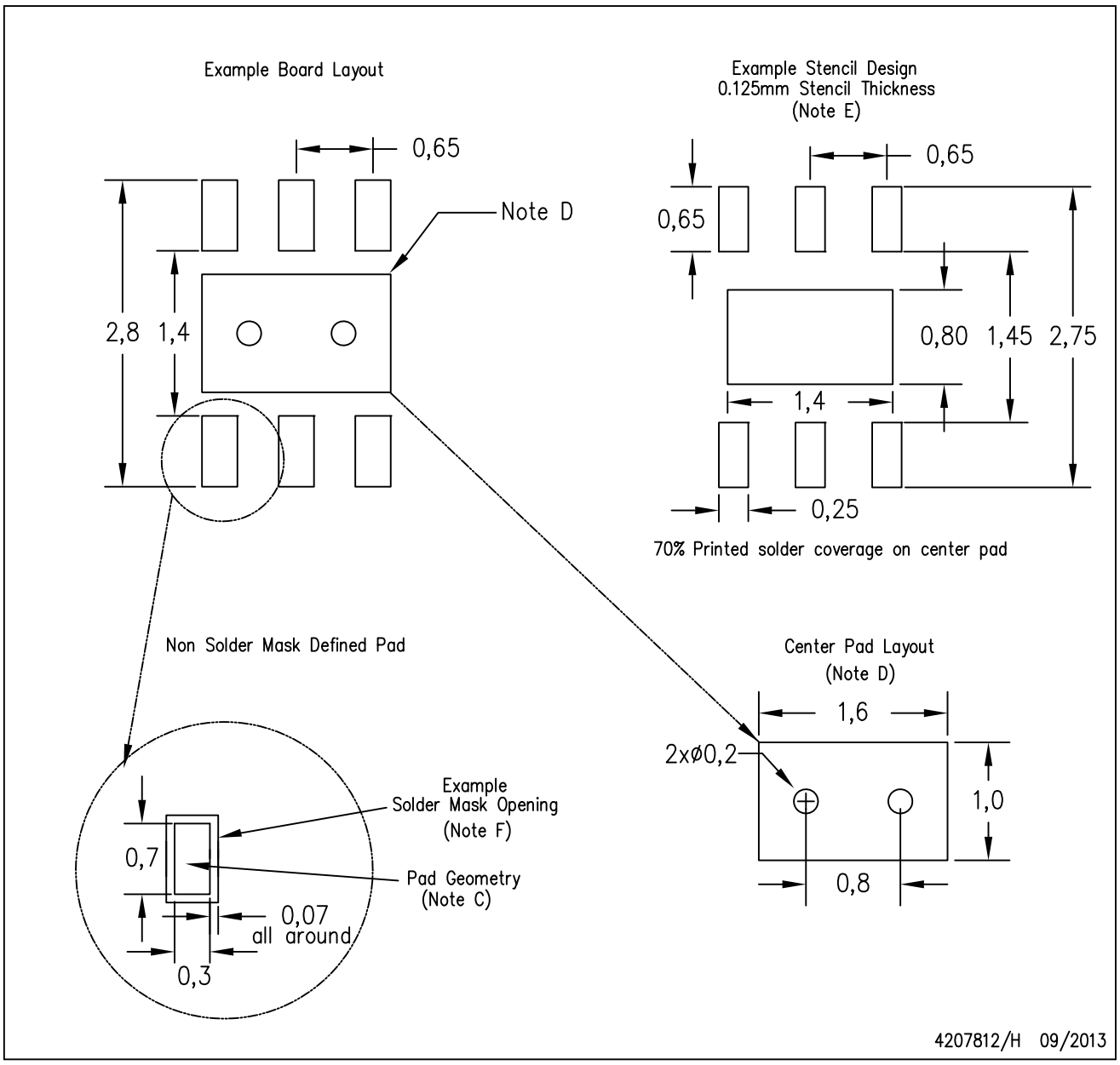
Bottom View

Exposed Thermal Pad Dimensions

4206926/N 03/13

NOTE: All linear dimensions are in millimeters

DRV (S–PWSON–N6) PLASTIC SMALL OUTLINE NO–LEAD



NOTES:
A. All linear dimensions are in millimeters.
B. This drawing is subject to change without notice.
C. Publication IPC–7351 is recommended for alternate designs.
D. This package is designed to be soldered to a thermal pad on the board. Refer to Application Note, QFN/SON PCB Attachment, Texas Instruments Literature No. SLUA271, and also the Product Data Sheets for specific thermal information, via requirements, and recommended board layout. These documents are available at www.ti.com <http://www.ti.com>.
E. Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC 7525 for stencil design considerations.
F. Customers should contact their board fabrication site for solder mask tolerances.

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